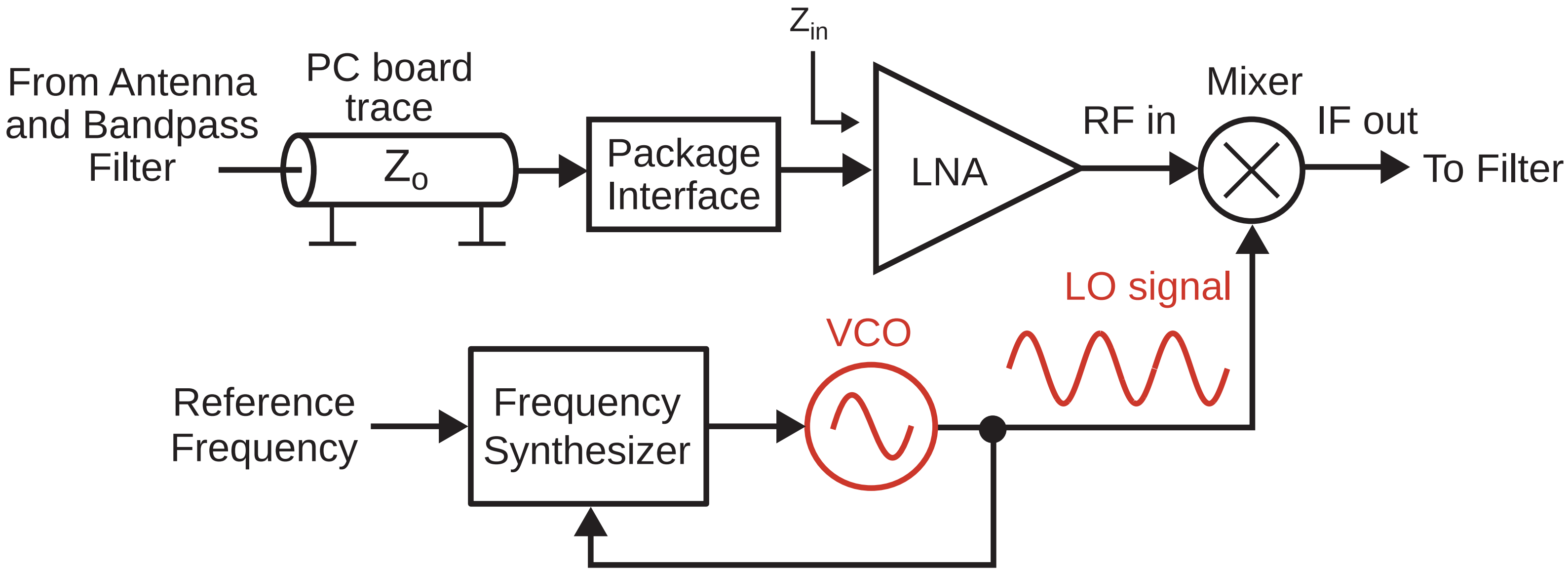
6.776
High Speed Communication Circuits and Systems
Lecture 14
Voltage Controlled Oscillators

Massachusetts Institute of Technology

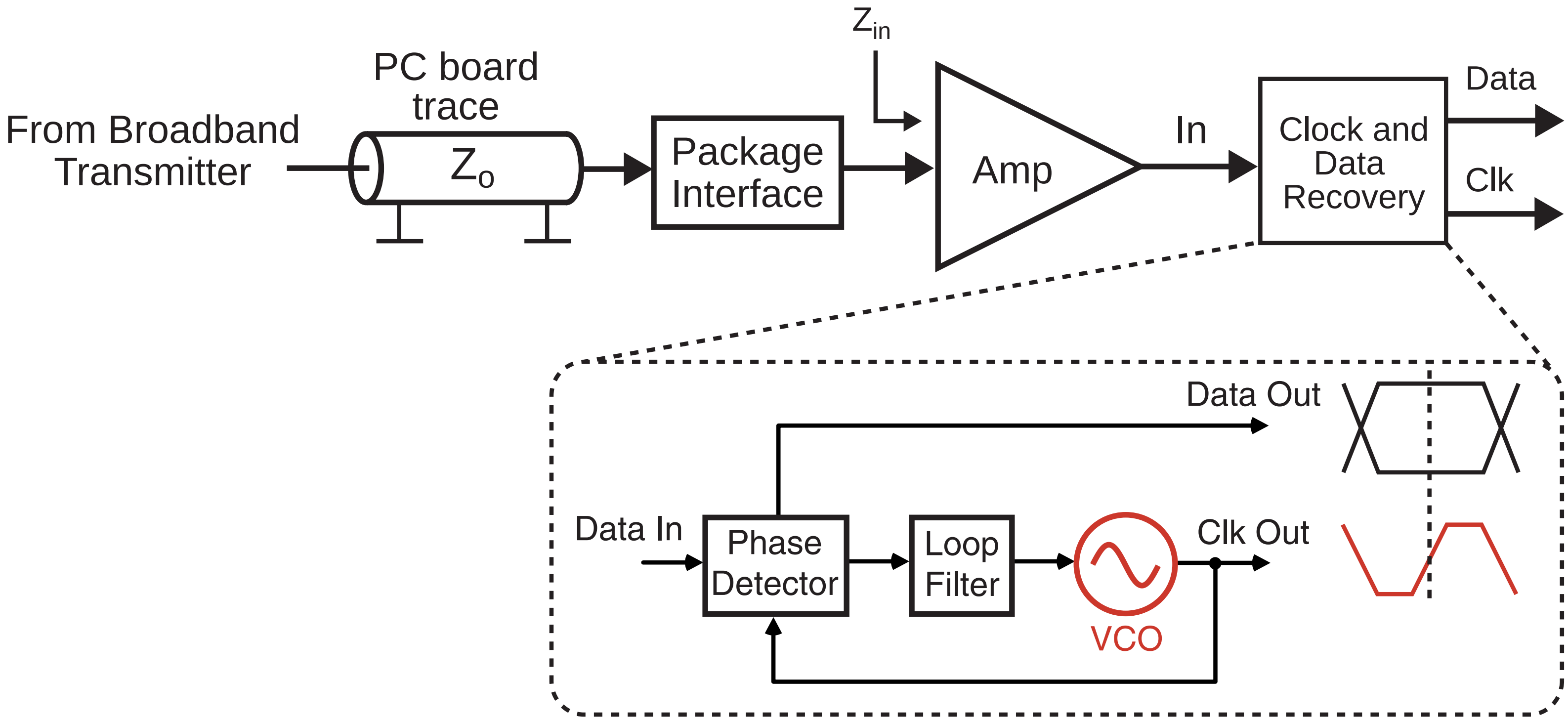
March 29, 2005

VCO Design for Narrowband Wireless Systems



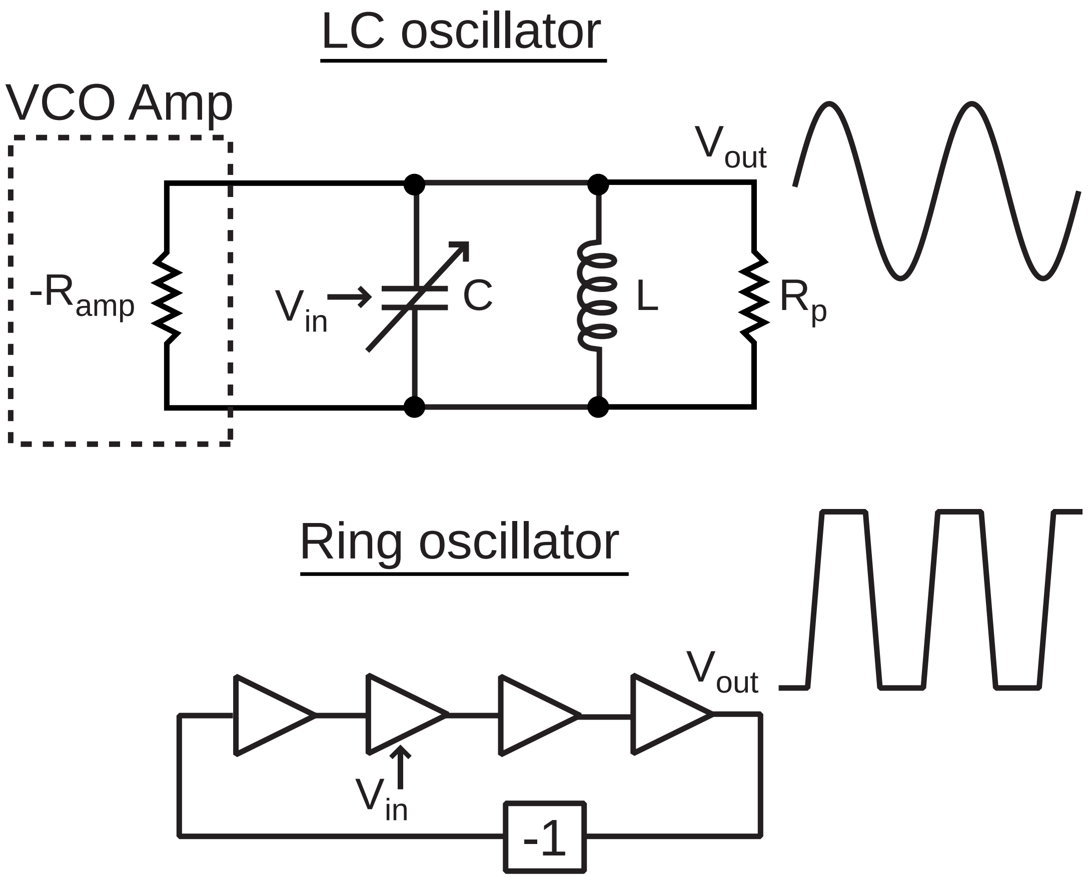
- **Design Issues**
  - **Tuning Range – need to cover all frequency channels**
  - **Noise – impacts receiver sensitivity performance**
  - **Power – want low power dissipation**
  - **Isolation – want to minimize noise pathways into VCO**
  - **Sensitivity to process/temp variations – need to make it manufacturable in high volume**

VCO Design For Broadband High Speed Data Links



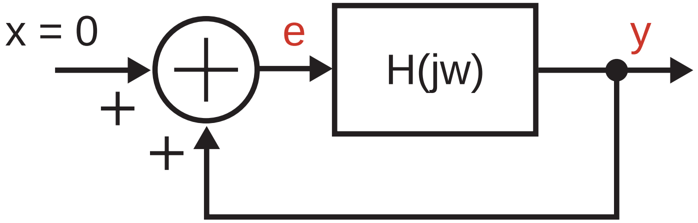
- **Design Issues**
  - **Same as wireless, but:**
    - Required noise performance is often less stringent
    - Tuning range is often narrower

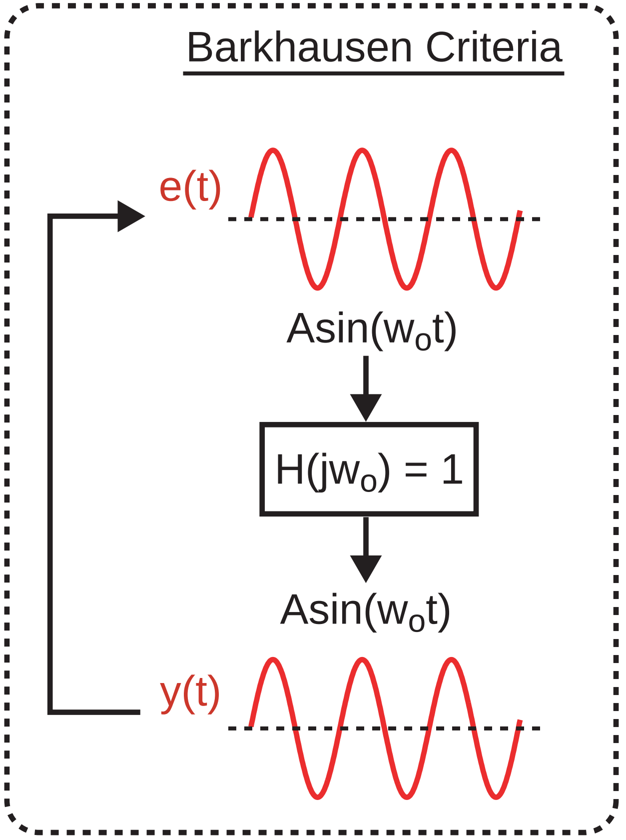
Popular VCO Structures



- **LC Oscillator: low phase noise, large area**
- **Ring Oscillator: easy to integrate, higher phase noise**

Barkhausen's Criteria for Oscillation





- **Closed loop transfer function**

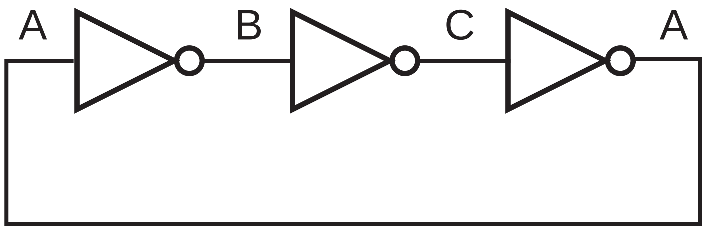
$$G(jw) = \frac{Y(jw)}{X(jw)} = \frac{H(jw)}{1 - H(jw)}$$

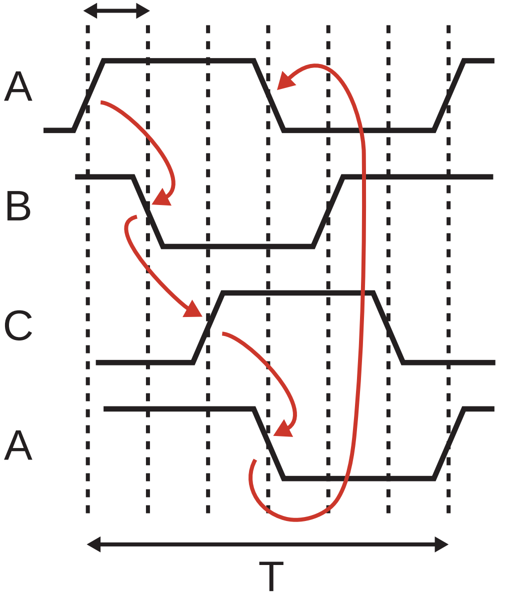
- **Self-sustaining oscillation at frequency ω_o if**

$$H(jw_o) = 1$$

  - **Amounts to two conditions:**
    - Gain = 1 at frequency ω_o
    - Phase = n360 degrees (n = 0,1,2,…) at frequency ω_o

Example 1: Ring Oscillator





- Gain is set to 1 by saturating characteristic of inverters
- Odd number of stages to prevent stable DC operating point
- Phase equals 360 degrees at frequency of oscillation (180 from inversion, another 180 from gate delays)
  - Assume N stages each with phase shift $\Delta\Phi$

$$N\Delta\Phi = 180^o \Rightarrow \Delta\Phi = \frac{180^o}{N}$$

  - Alternately, N stages with delay Δt

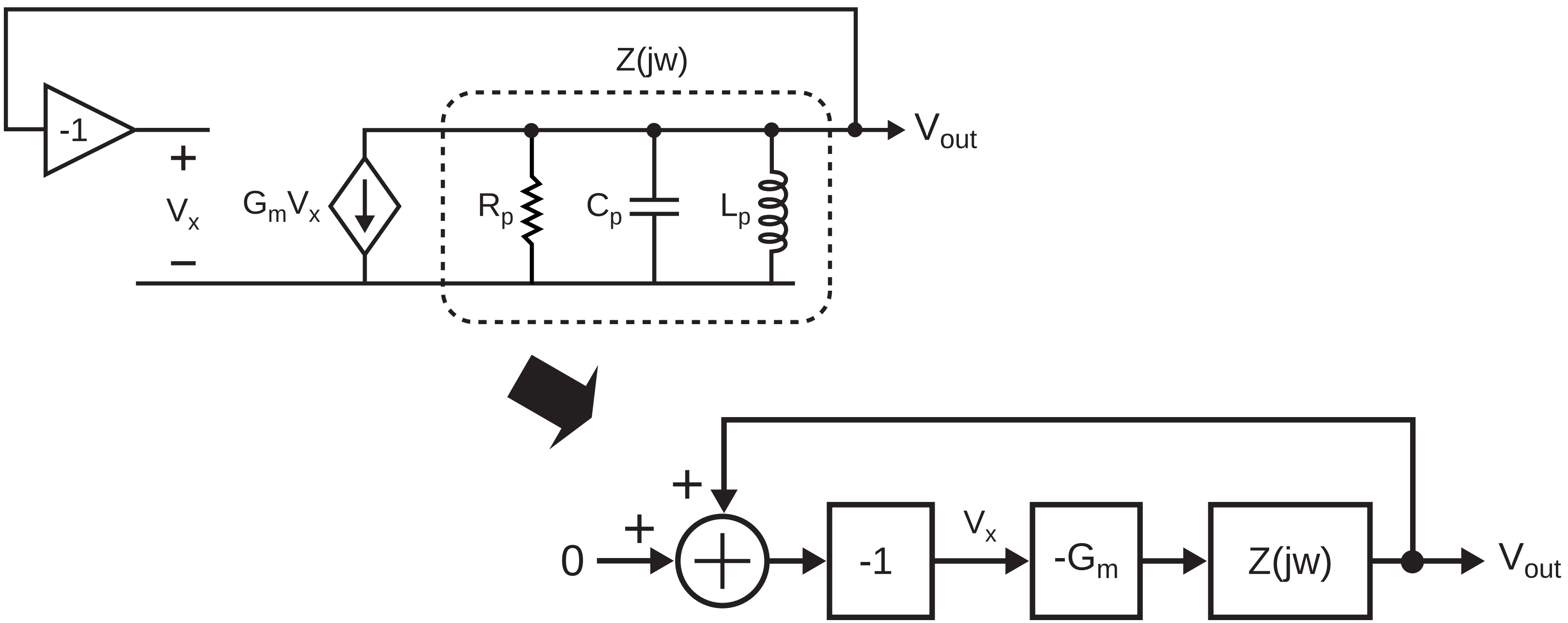
$$N\Delta t = \frac{T}{2} \Rightarrow \Delta t = \frac{T/2}{N}$$

Further Info on Ring Oscillators

- Due to their relatively poor phase noise performance, ring oscillators are rarely used in RF systems
  - They are used quite often in high speed data links,
  - We will focus on LC oscillators in this lecture

- Some useful info on CMOS ring oscillators
  - Maneatis et. al., "Precise Delay Generation Using Coupled Oscillators", JSSC, Dec 1993 (look at pp 127-128 for delay cell description)
  - Todd Weigandt's PhD thesis – http://kabuki.eecs.berkeley.edu/~weigandt/

Example 2: Resonator-Based Oscillator



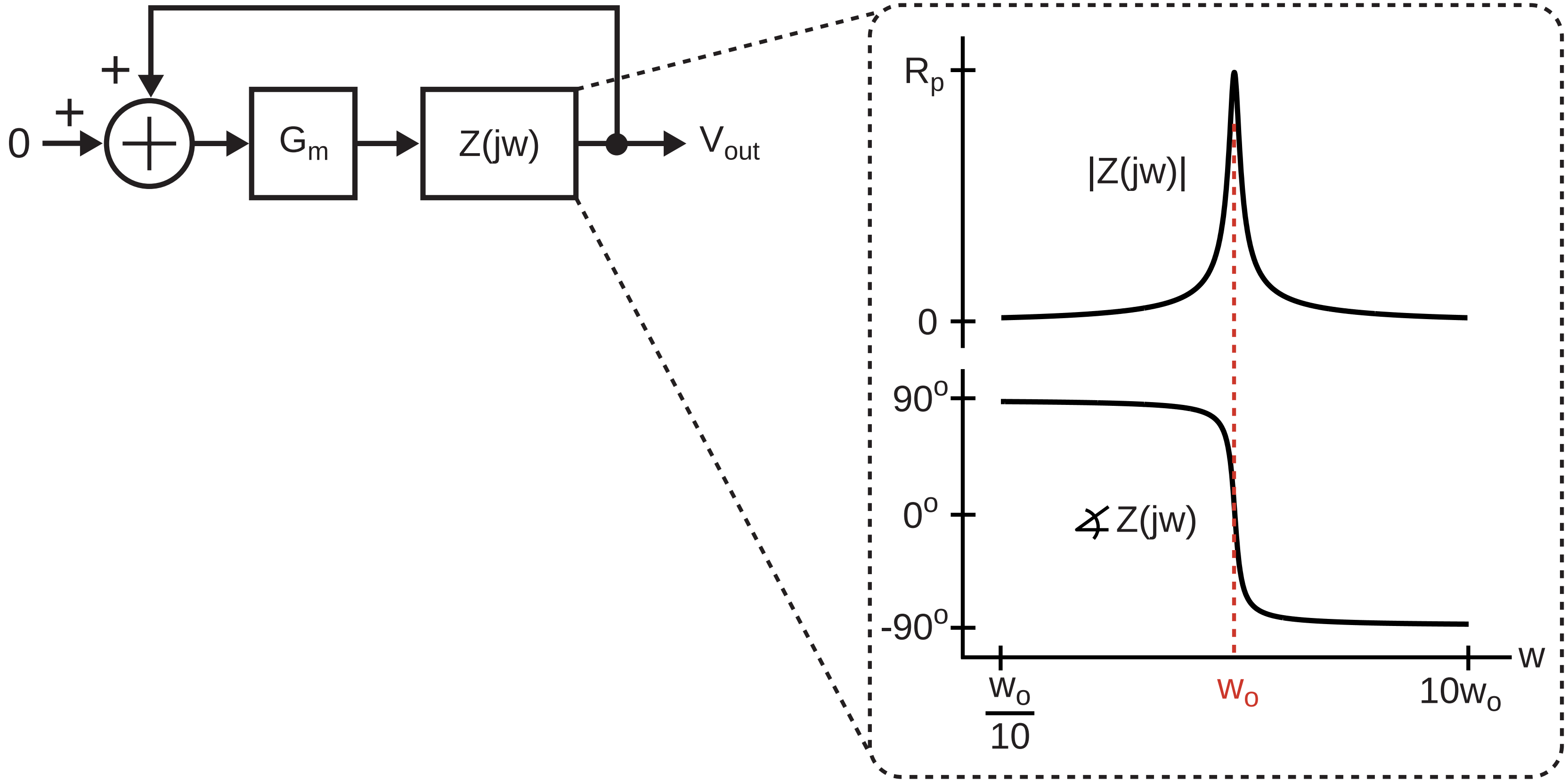
- **Barkhausen Criteria for oscillation at frequency ω_o:**

$$G_m Z(jw_o) = 1$$

  - **Assuming G_m is purely real, $Z(j\omega_o)$ must also be purely real**

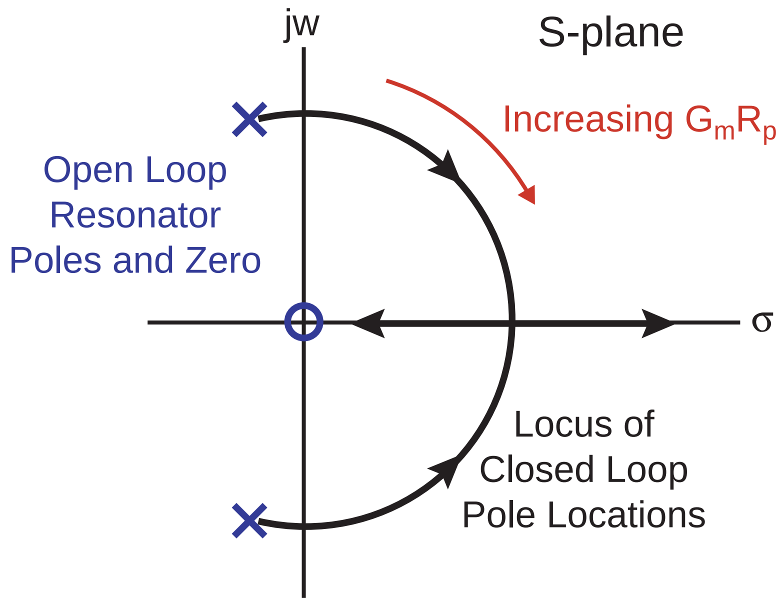
$$G_m R_p = 1$$

A Closer Look At Resonator-Based Oscillator



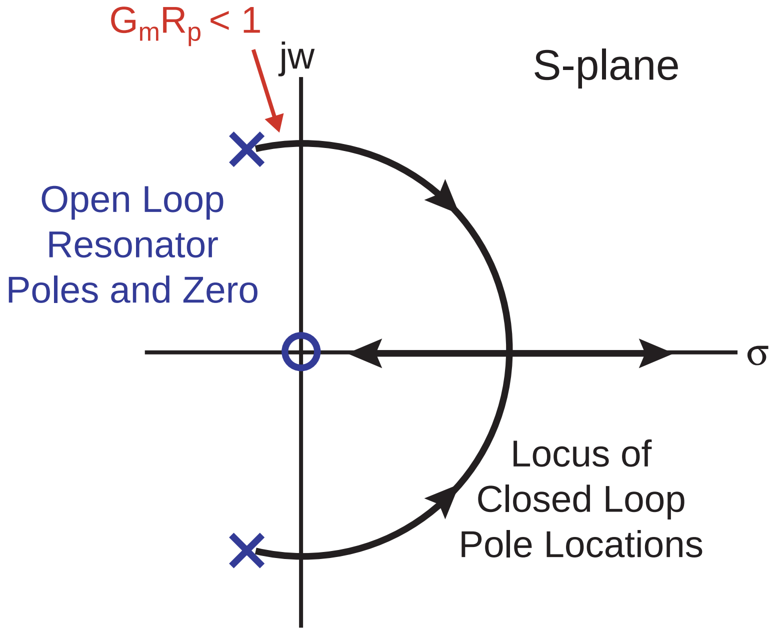
- **For parallel resonator at resonance**
  - **Looks like resistor (i.e., purely real) at resonance**
    - Phase condition is satisfied
    - Magnitude condition achieved by setting $G_m R_p = 1$

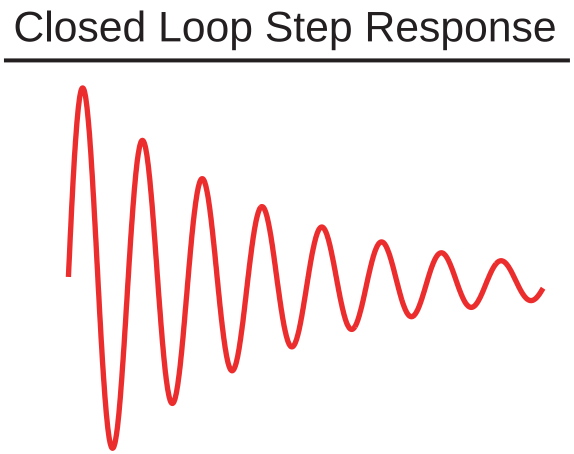
Impact of Different G_m Values



- **Root locus plot allows us to view closed loop pole locations as a function of open loop poles/zero and open loop gain (G_mR_p)**
  - **As gain (G_mR_p) increases, closed loop poles move into right half S-plane**

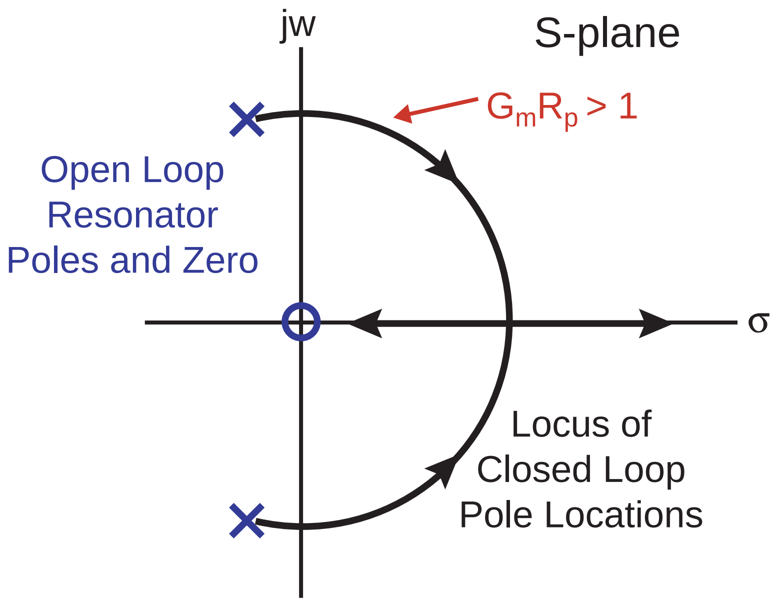
Impact of Setting G_m too low

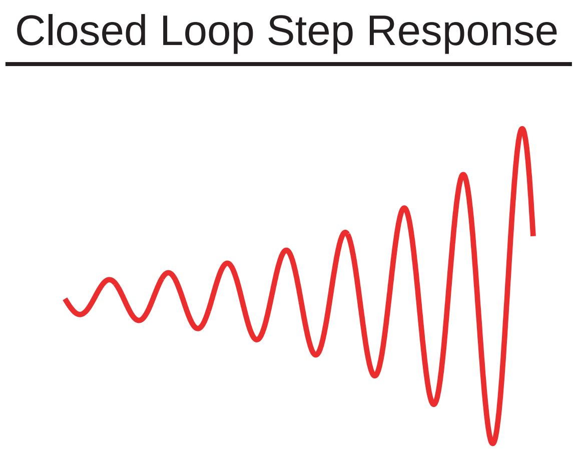




- **Closed loop poles end up in the left half S-plane**
  - **Underdamped response occurs**
    - Oscillation dies out

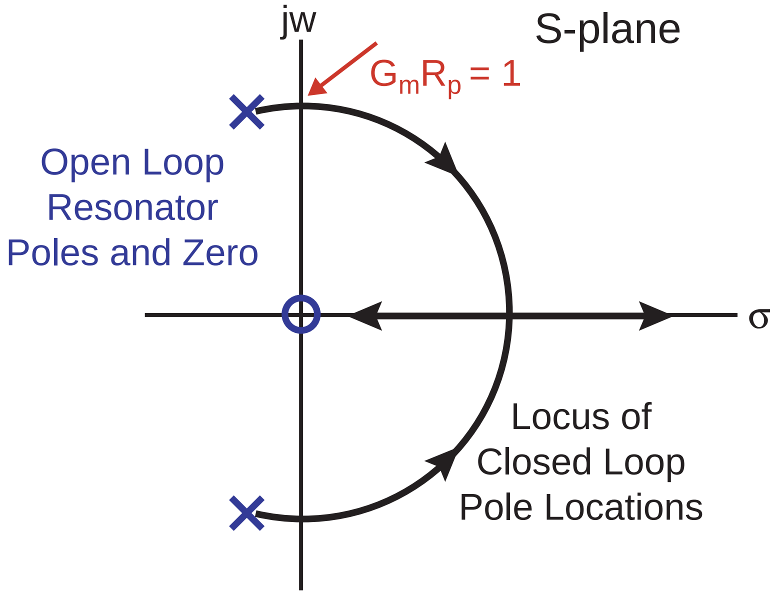
Impact of Setting G_m too High

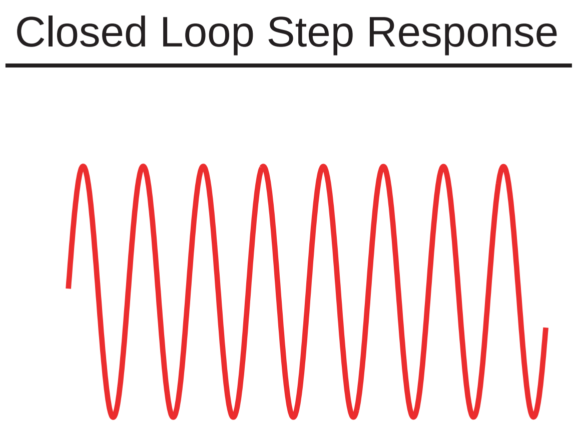




- **Closed loop poles end up in the right half S-plane**
  - **Unstable response occurs**
    - Waveform blows up!

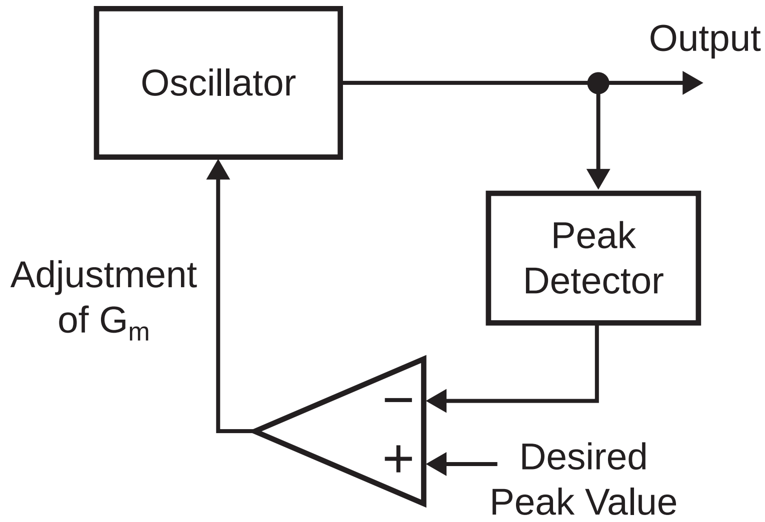
Setting G_m To Just the Right Value





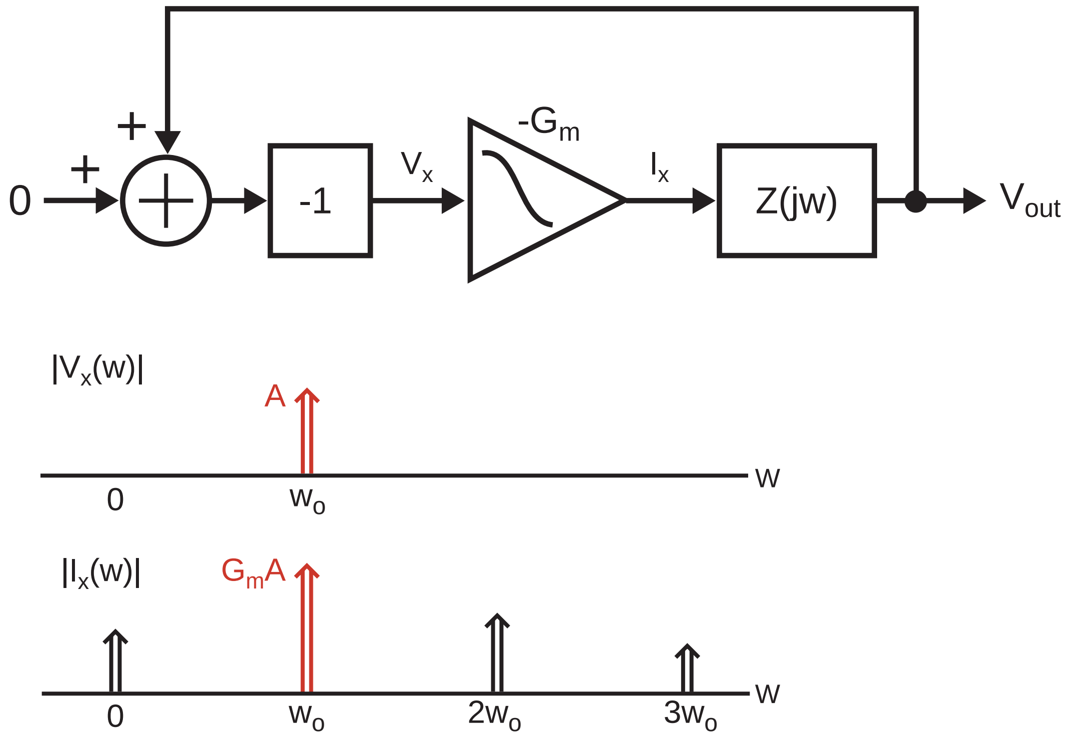
- **Closed loop poles end up on jw axis**
  - **Oscillation maintained**
- **Issue – G_mR_p needs to *exactly* equal 1**
  - **How do we achieve this in practice?**

Amplitude Feedback Loop



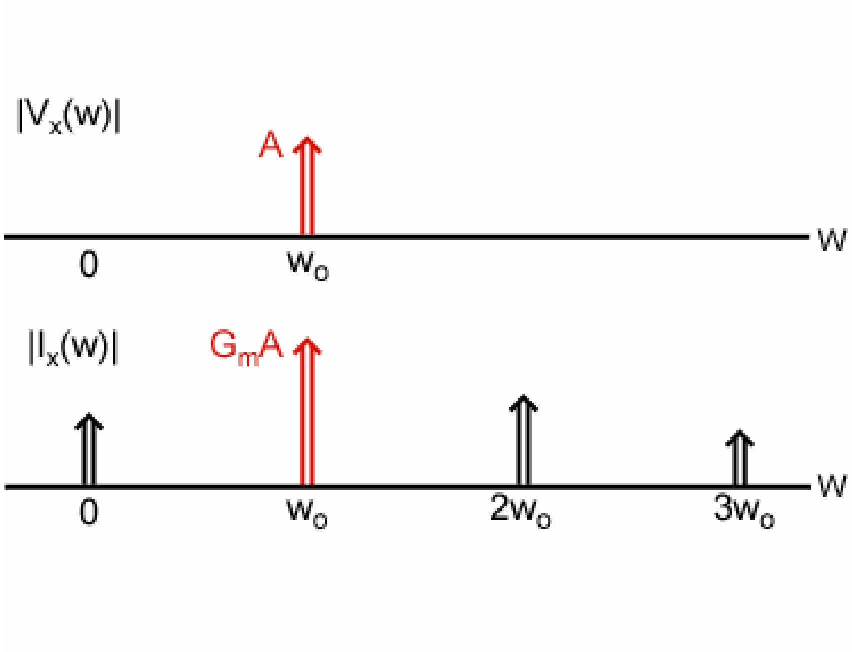
- **One thought is to detect oscillator amplitude, and then adjust G_m so that it equals a desired value**
  - **By using feedback, we can precisely achieve $G_m R_p = 1$**
- **Issues**
  - **Complex, requires power, and adds noise**

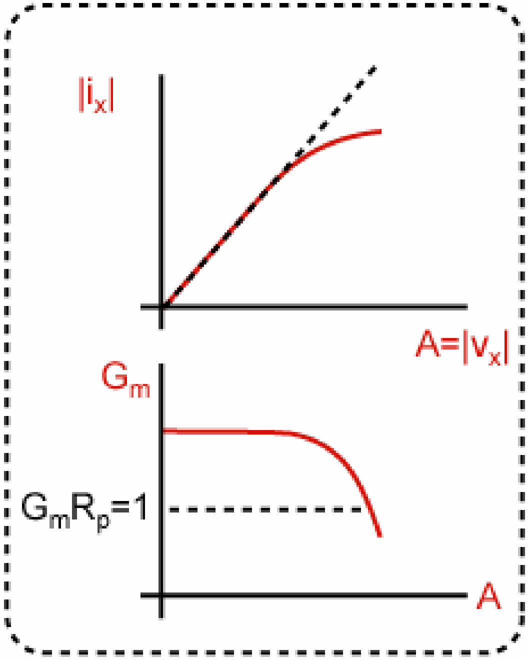
Leveraging Amplifier Nonlinearity as Feedback



- **Practical transconductance amplifiers have saturating characteristics**
  - **Harmonics created, but filtered out by resonator**
  - **Our interest is in the relationship between the input and the fundamental of the output**

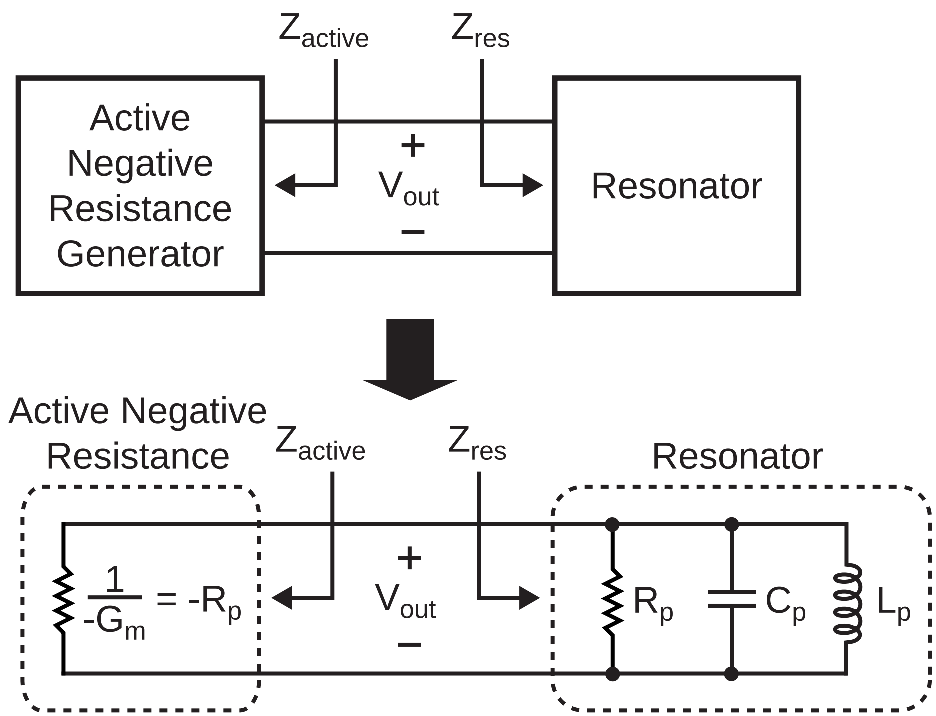
Amplifier Nonlinearity as Amplitude Control





- **As input amplitude is increased**
  - **Effective gain from input to fundamental of output drops**
  - **Amplitude feedback occurs! (G_mR_p = 1 in steady-state)**

One-Port View of Resonator-Based Oscillators

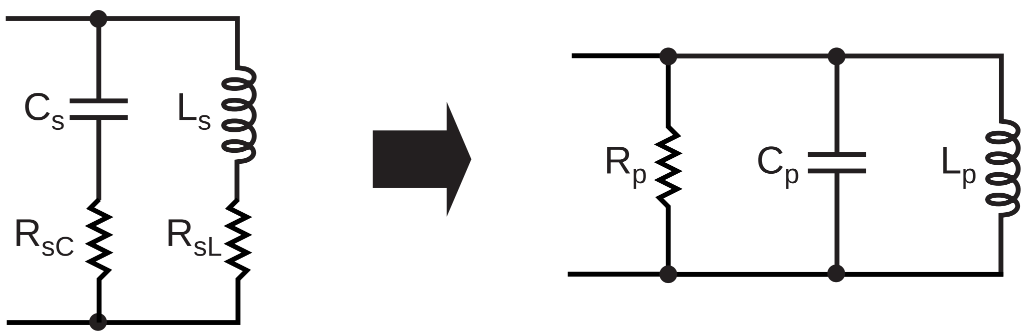


- Convenient for intuitive analysis
- Here we seek to cancel out loss in tank with a negative resistance element
  - To achieve sustained oscillation, we must have

$$\frac{1}{G_m} = R_p \quad \Rightarrow \quad G_m R_p = 1$$

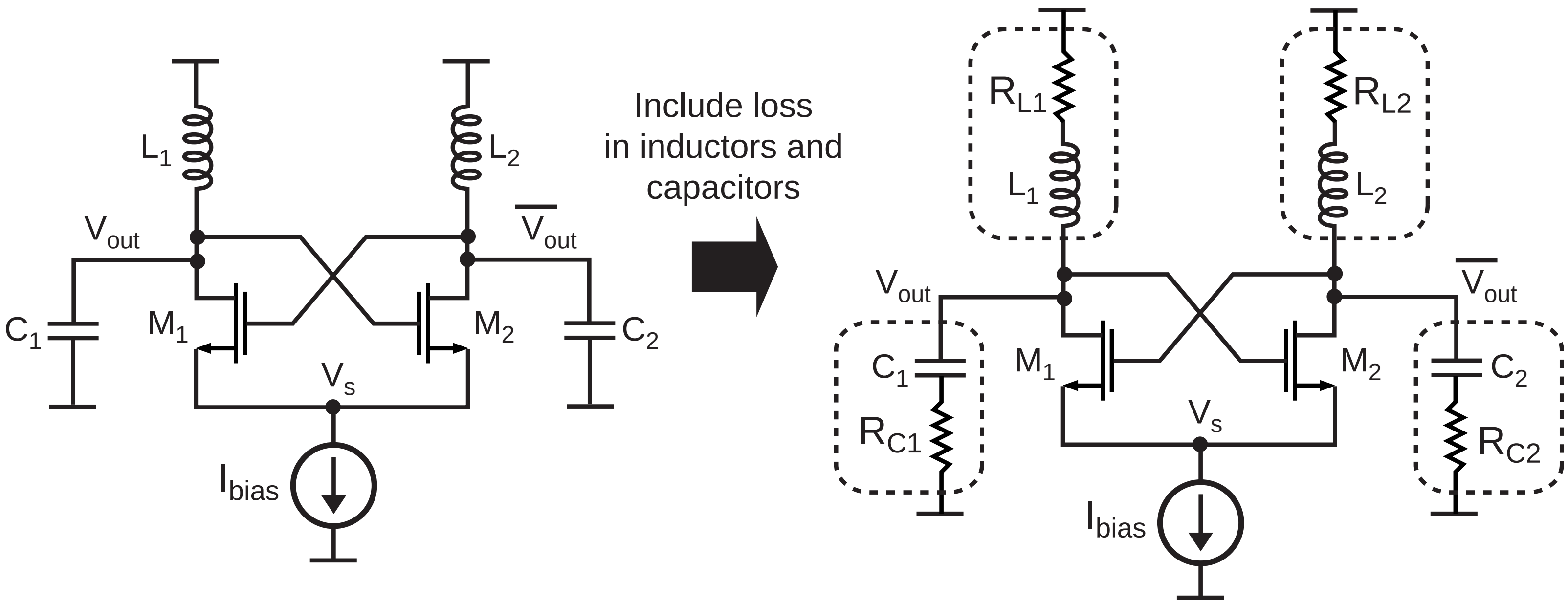
One-Port Modeling Requires Parallel RLC Network

- **Since VCO operates over a very narrow band of frequencies, we can always do series to parallel transformations to achieve a parallel network for analysis**



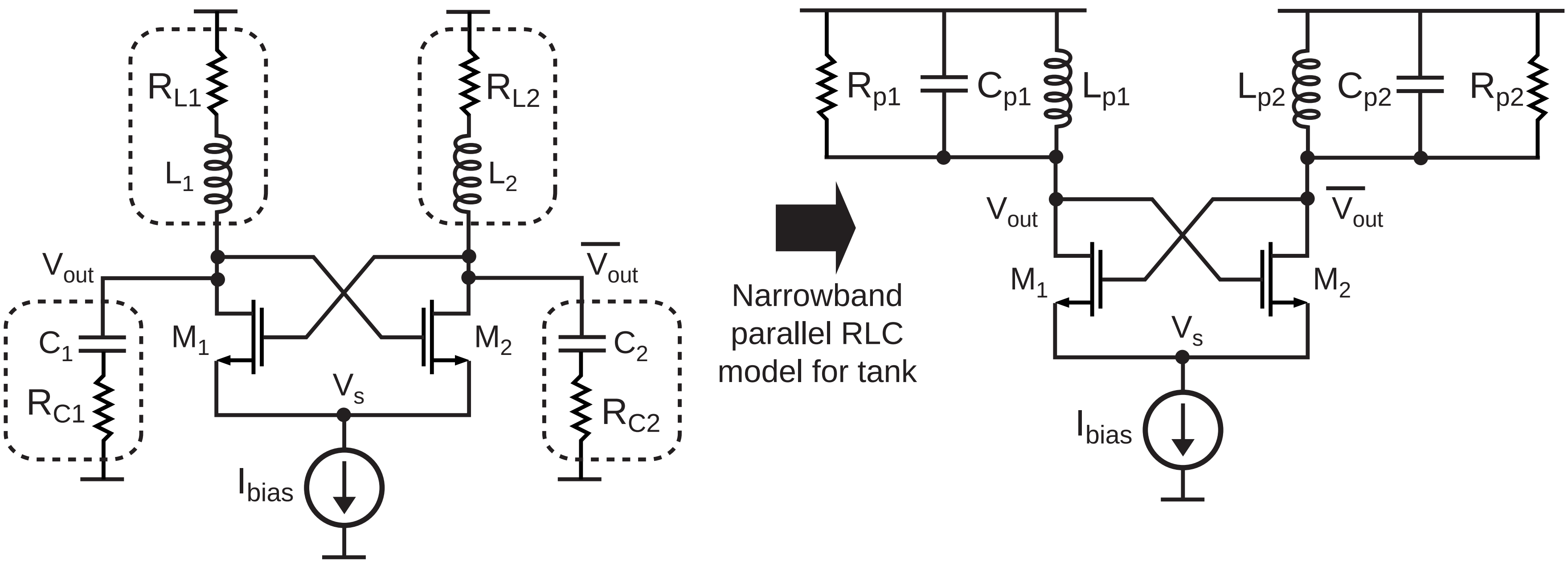
  - **Warning – in practice, RLC networks can have secondary (or more) resonant frequencies, which cause undesirable behavior**
    - Equivalent parallel network masks this problem in hand analysis
    - Simulation will reveal the problem

VCO Example – Negative Resistance Oscillator



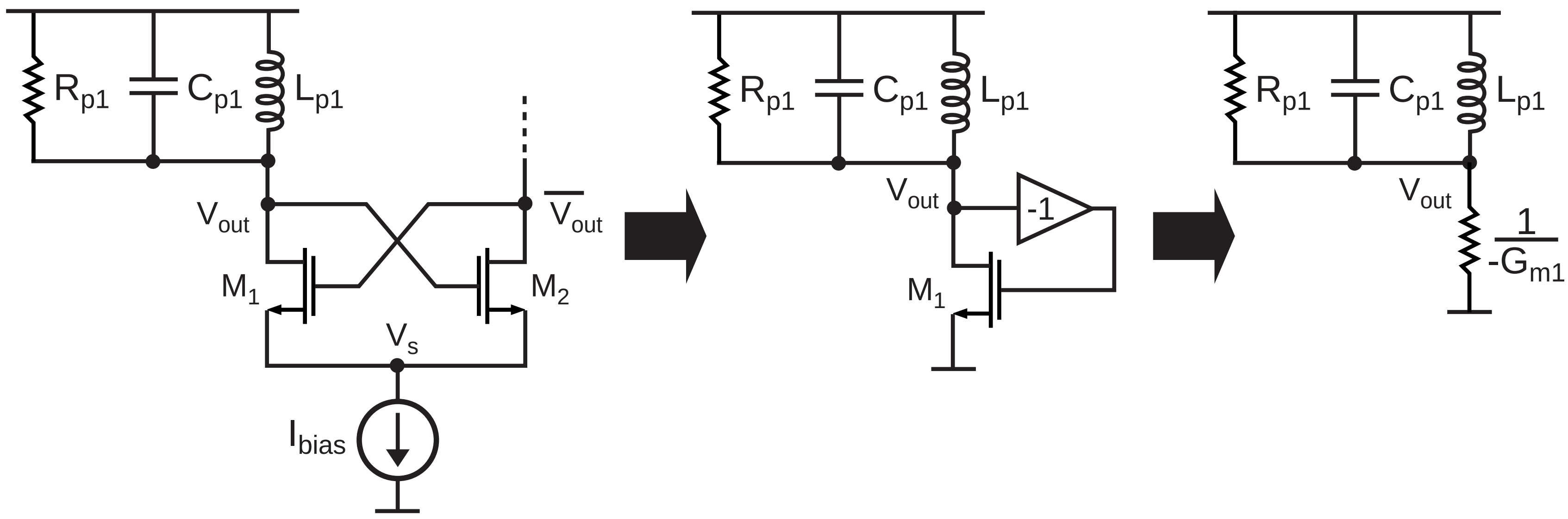
- **This type of oscillator structure is quite popular in current CMOS implementations**
  - **Advantages**
    - Simple topology
    - Differential implementation (good for feeding differential circuits)
    - Good phase noise performance can be achieved

Analysis of Negative Resistance Oscillator (Step 1)



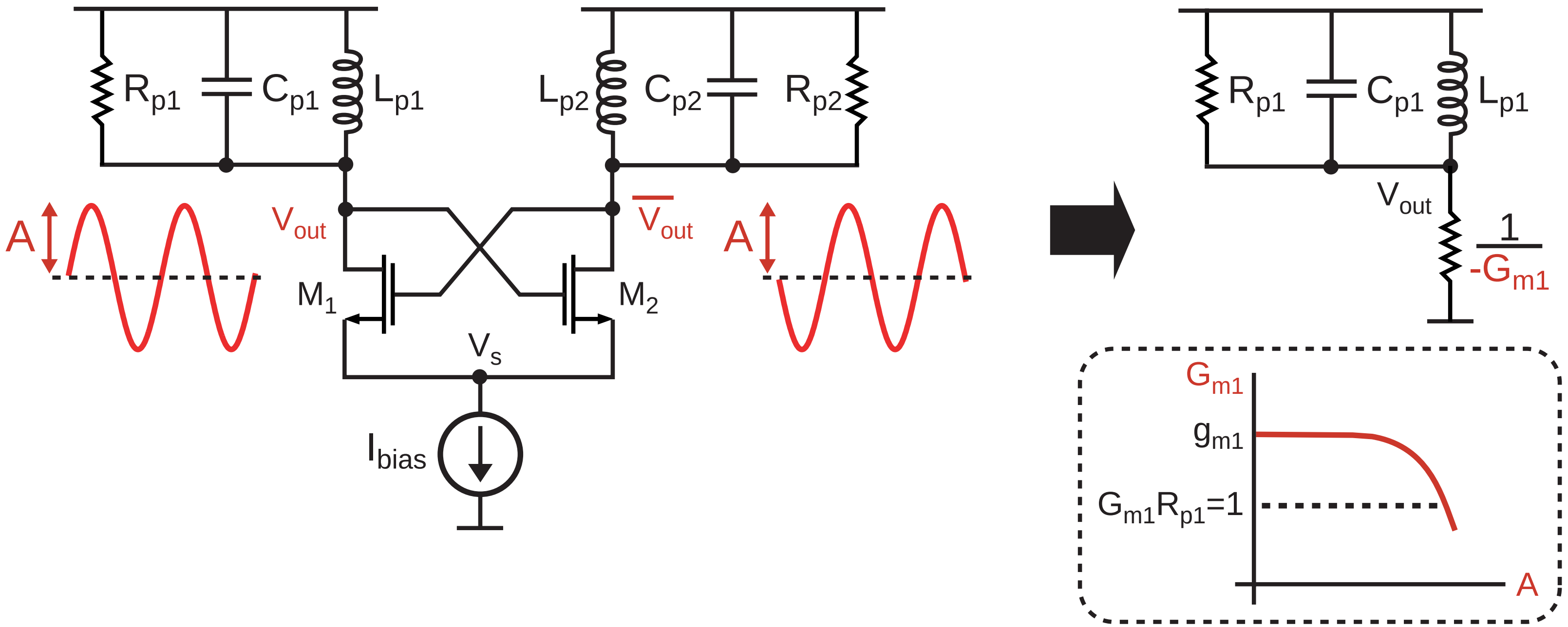
- **Derive a parallel RLC network that includes the loss of the tank inductor and capacitor**
  - **Typically, such loss is dominated by series resistance in the inductor**

Analysis of Negative Resistance Oscillator (Step 2)



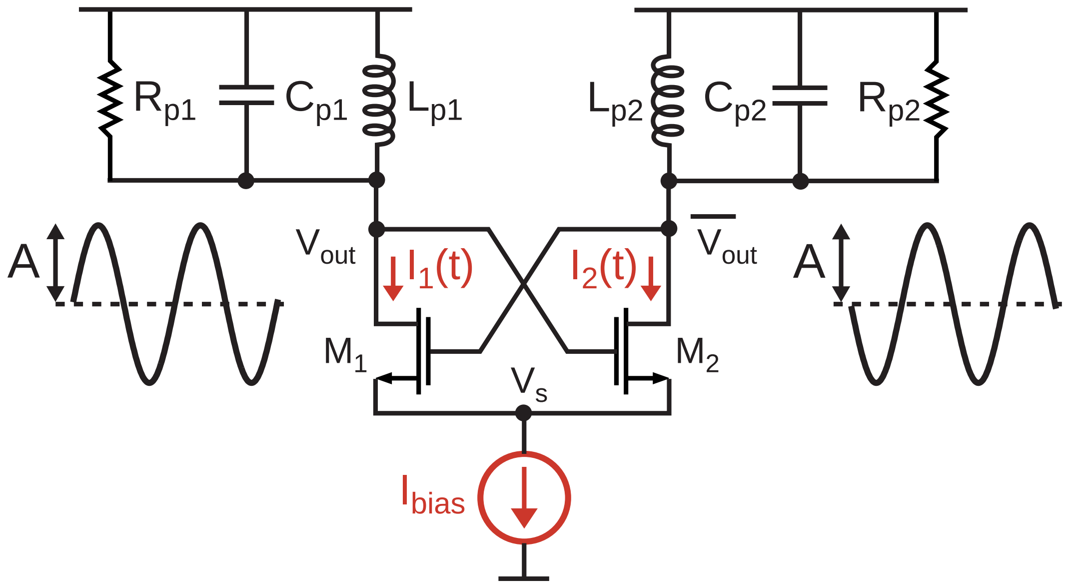
- **Split oscillator circuit into half circuits to simplify analysis**
  - **Leverages the fact that we can approximate V_s as being incremental ground (this is not quite true, but close enough)**
- **Recognize that we have a diode connected device with a negative transconductance value**
  - **Replace with negative resistor**
    - Note: G_m is ***large signal*** transconductance value

Design of Negative Resistance Oscillator



- **Design tank components to achieve high Q**
  - **Resulting R_p value is as large as possible**
- **Choose bias current (I_{bias}) for large swing (without going far into G_m saturation)**
  - **We'll estimate swing as a function of I_{bias} shortly**
- **Choose transistor size to achieve adequately large g_{m1}**
  - **Usually twice as large as $1/R_{p1}$ to guarantee startup**

Calculation of Oscillator Swing: Max. Sinusoidal Oscillation



- If we assume the amplitude is large, I_{bias} is fully steered to one side at the peak and the bottom of the sinusoid:

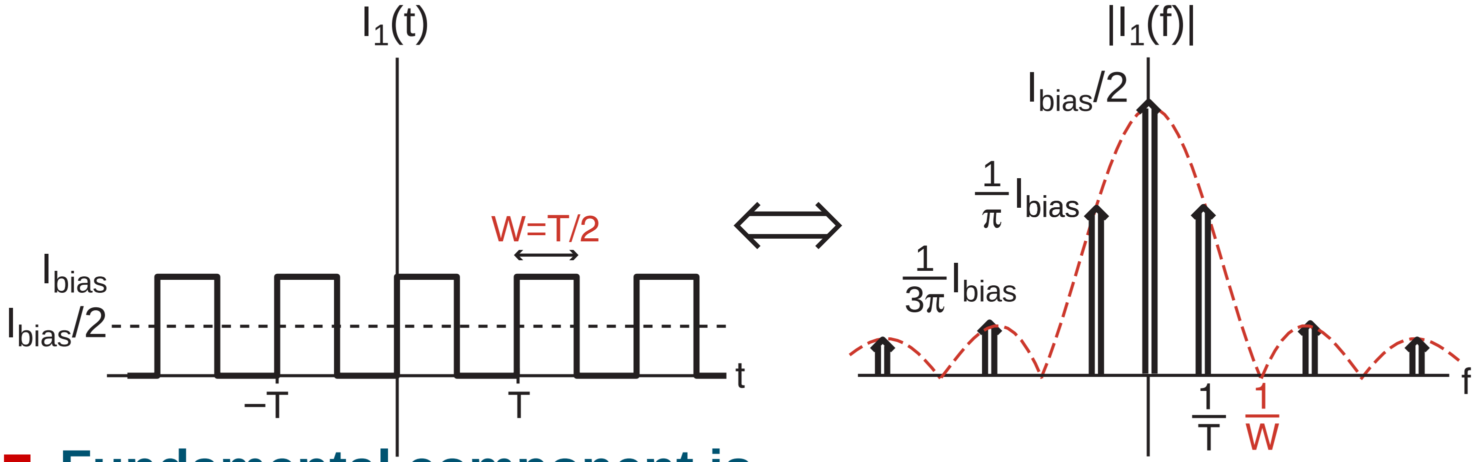
$$i_1(t), i_2(t) > 0 \qquad i_1(t) + i_2(t) = I_{bias}$$

$$i_1(t) = \frac{I_{bias}}{2}(sinw_o t + 1) \quad i_2(t) = \frac{I_{bias}}{2}(-sinw_o t + 1)$$

$$A = \frac{1}{2} I_{bias} R_p$$

Calculation of Oscillator Swing: Squarewave Oscillation

- **If amplitude is very large, we can assume $I_1(t)$ is a square wave**
  - **We are interested in determining fundamental component**
    - (DC and harmonics filtered by tank)



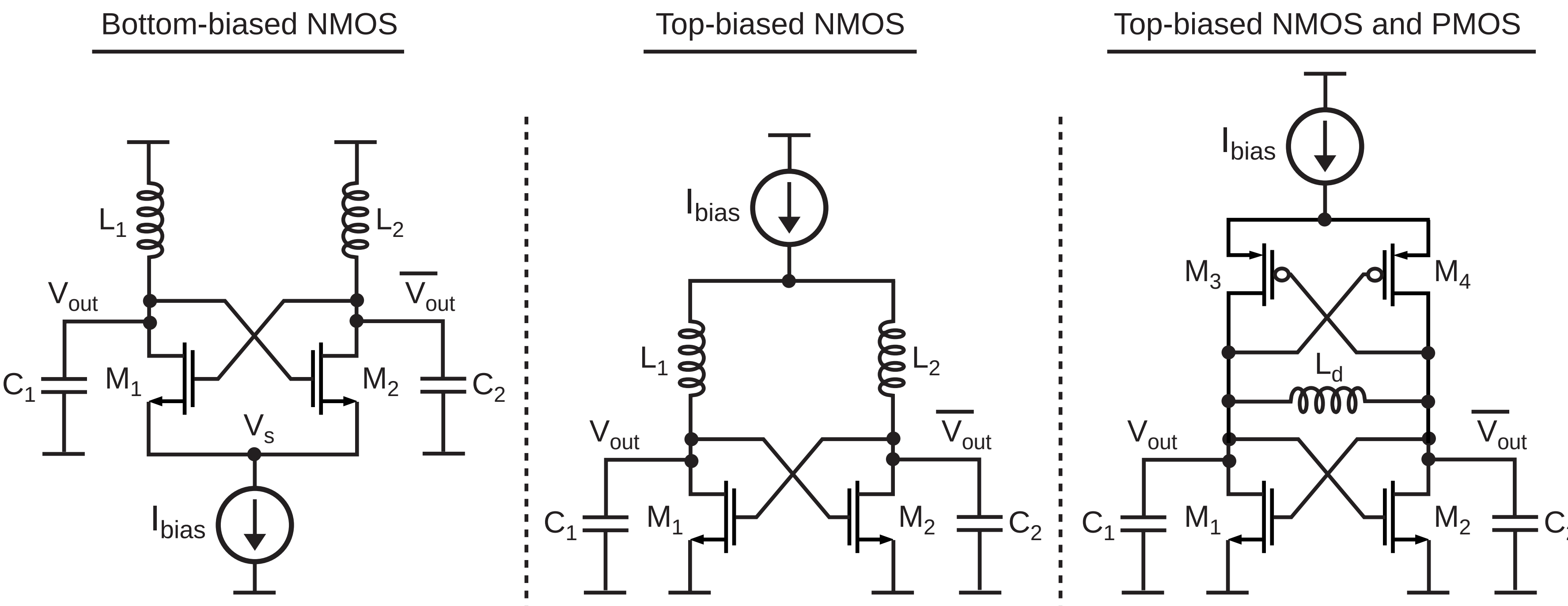
  - **Fundamental component is**

$$I_1(t)\Big|_{fund} = \frac{2}{\pi} I_{bias} \sin(w_o t), \quad \text{where} \quad w_o = \frac{2\pi}{T}$$

  - **Resulting oscillator amplitude**

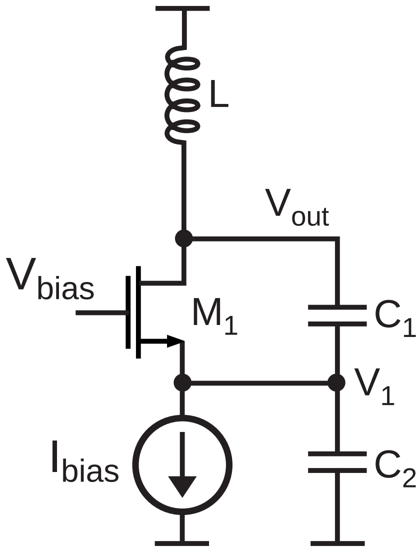
$$A = \frac{2}{\pi} I_{bias} R_p$$

Variations on a Theme



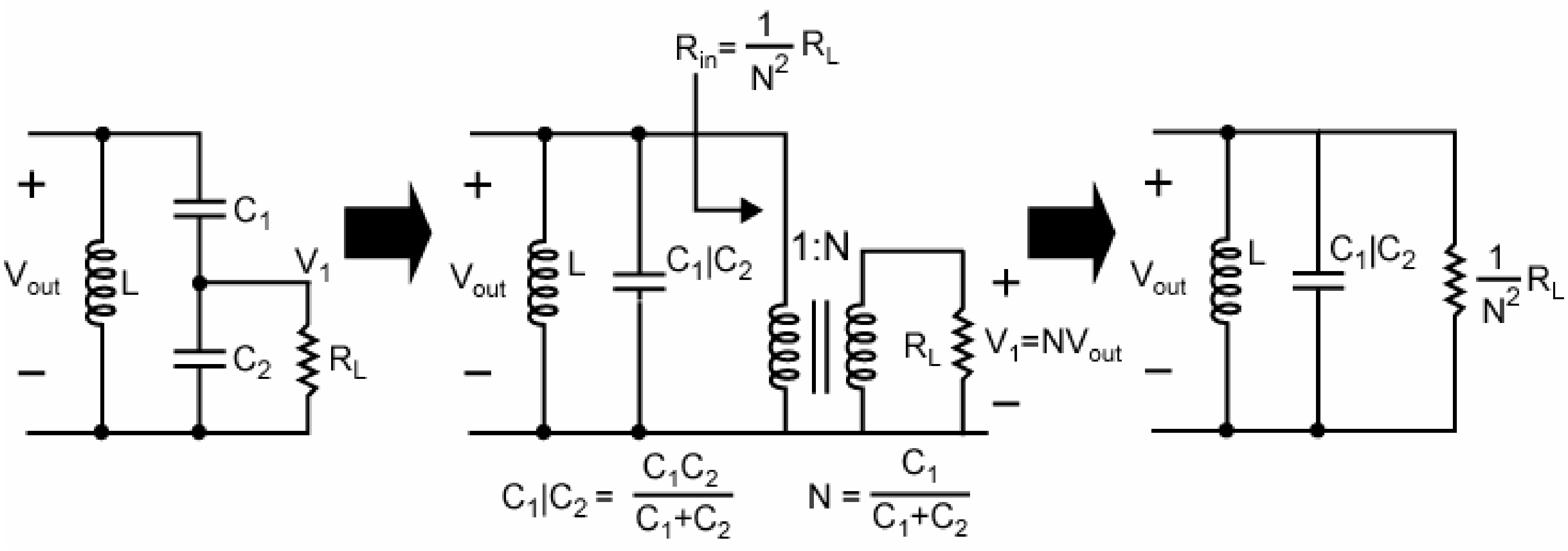
- **Biasing can come from top or bottom**
- **Can use either NMOS, PMOS, or both for transconductor**
  - **Use of both NMOS and PMOS for coupled pair would appear to achieve better phase noise at a given power dissipation**
    - See Hajimiri et. al, “Design Issues in CMOS Differential LC Oscillators”, JSSC, May 1999 and Feb, 2000 (pp 286-287)

Colpitts Oscillator



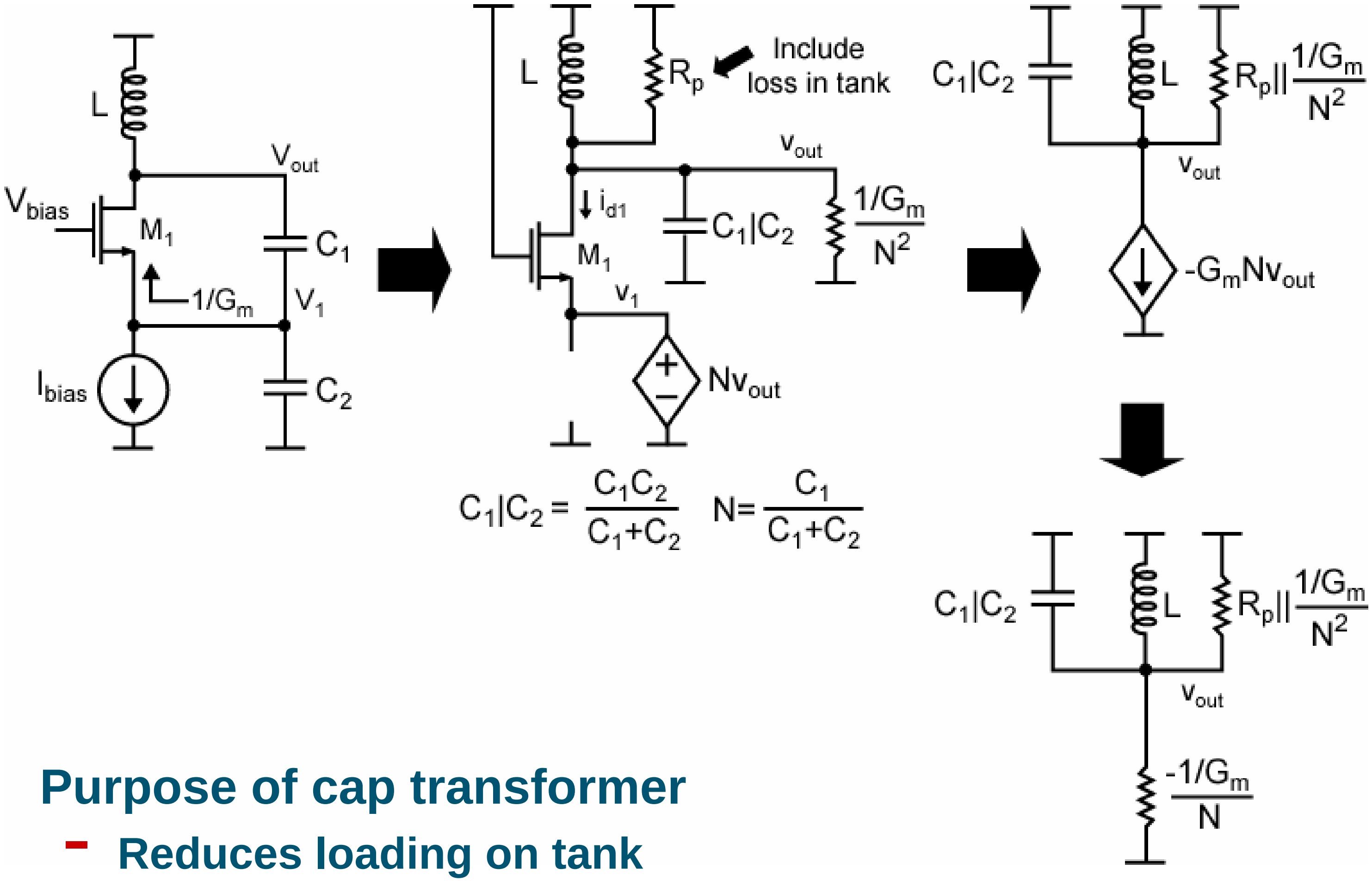
- **Carryover from discrete designs in which single-ended approaches were preferred for simplicity**
  - **Achieves negative resistance with only one transistor**
  - **Differential structure can also be implemented, though**
- **Good phase noise can be achieved, but not apparent there is an advantage of this design over negative resistance design for CMOS applications**

Analysis of Cap Transformer used in Colpitts



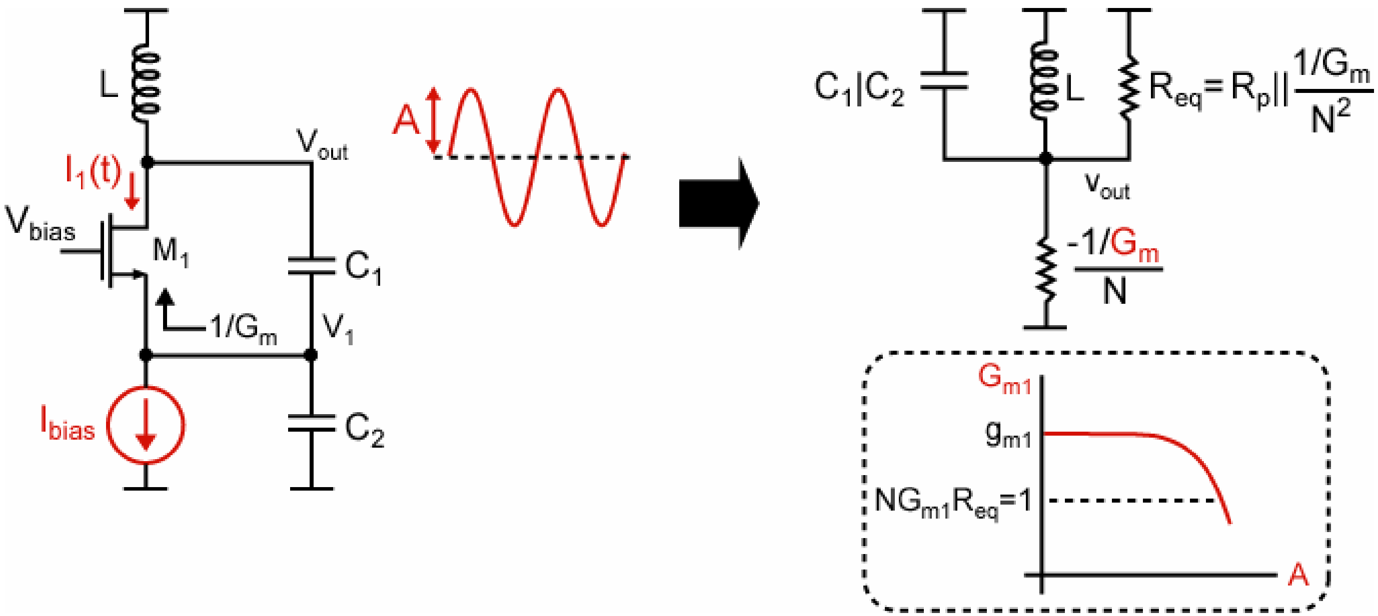
- **Voltage drop across R_L is reduced by capacitive voltage divider**
  - **Assume that impedances of caps are less than R_L at resonant frequency of tank (simplifies analysis)**
    - Ratio of V_1 to V_{out} set by caps and not R_L
- **Power conservation leads to transformer relationship shown (See Lecture 4)**

Simplified Model of Colpitts



- **Purpose of cap transformer**
  - **Reduces loading on tank**
  - **Reduces swing at source node (important for bipolar version)**
- **Transformer ratio set to achieve best noise performance**

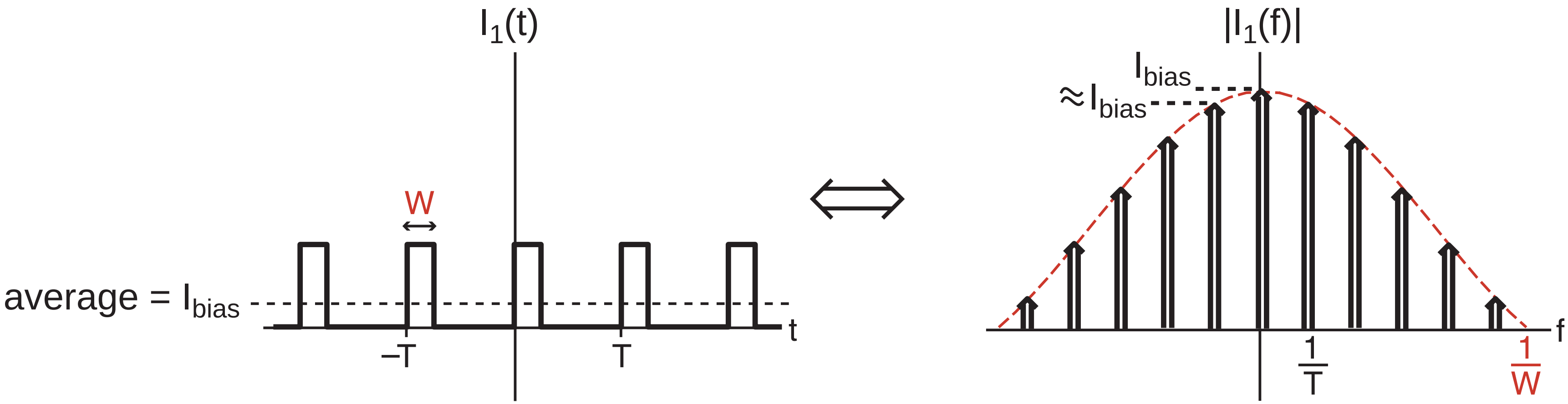
Design of Colpitts Oscillator



- Design tank for high Q
- Choose bias current (I_{bias}) for large swing (without going far into G_m saturation)
- Choose transformer ratio for best noise
  - Rule of thumb: choose N = 1/5 according to Tom Lee
- Choose transistor size to achieve adequately large g_{m1}

Calculation of Oscillator Swing as a Function of I_{bias}

- $I_1(t)$ consists of pulses whose shape and width are a function of the transistor behavior and transformer ratio
  - Approximate as narrow square wave pulses with width W



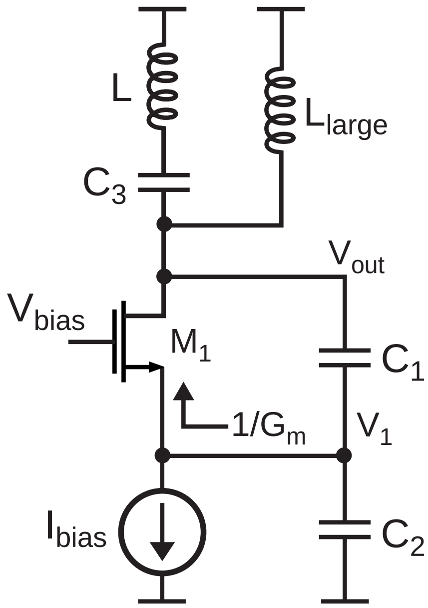
  - Fundamental component is

$$I_1(t)\Big|_{fund} \approx 2I_{bias}\sin(w_o t), \quad \text{where} \quad w_o = \frac{2\pi}{T}$$

  - Resulting oscillator amplitude

$$A \approx 2I_{bias}R_{eq}$$

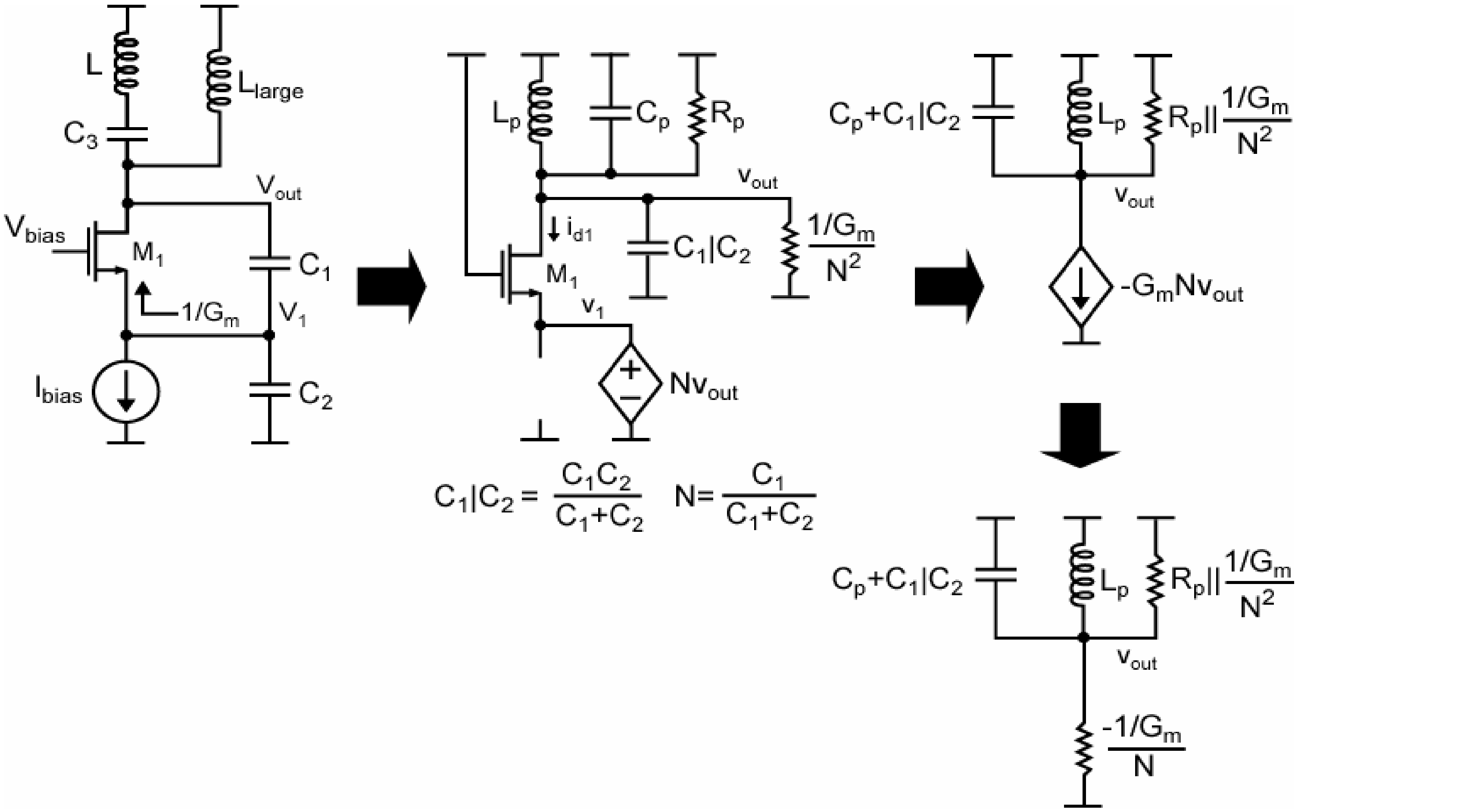
Clapp Oscillator



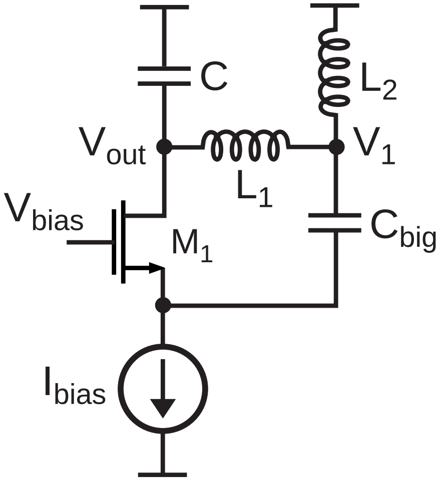
- **Same as Colpitts except that inductor portion of tank is isolated from the drain of the device**
  - **Allows inductor voltage to achieve a larger amplitude without exceeded the max allowable voltage at the drain**
    - Good for achieving lower phase noise

Simplified Model of Clapp Oscillator

- Looks similar to Colpitts model
  - Be careful of parasitic resonances!

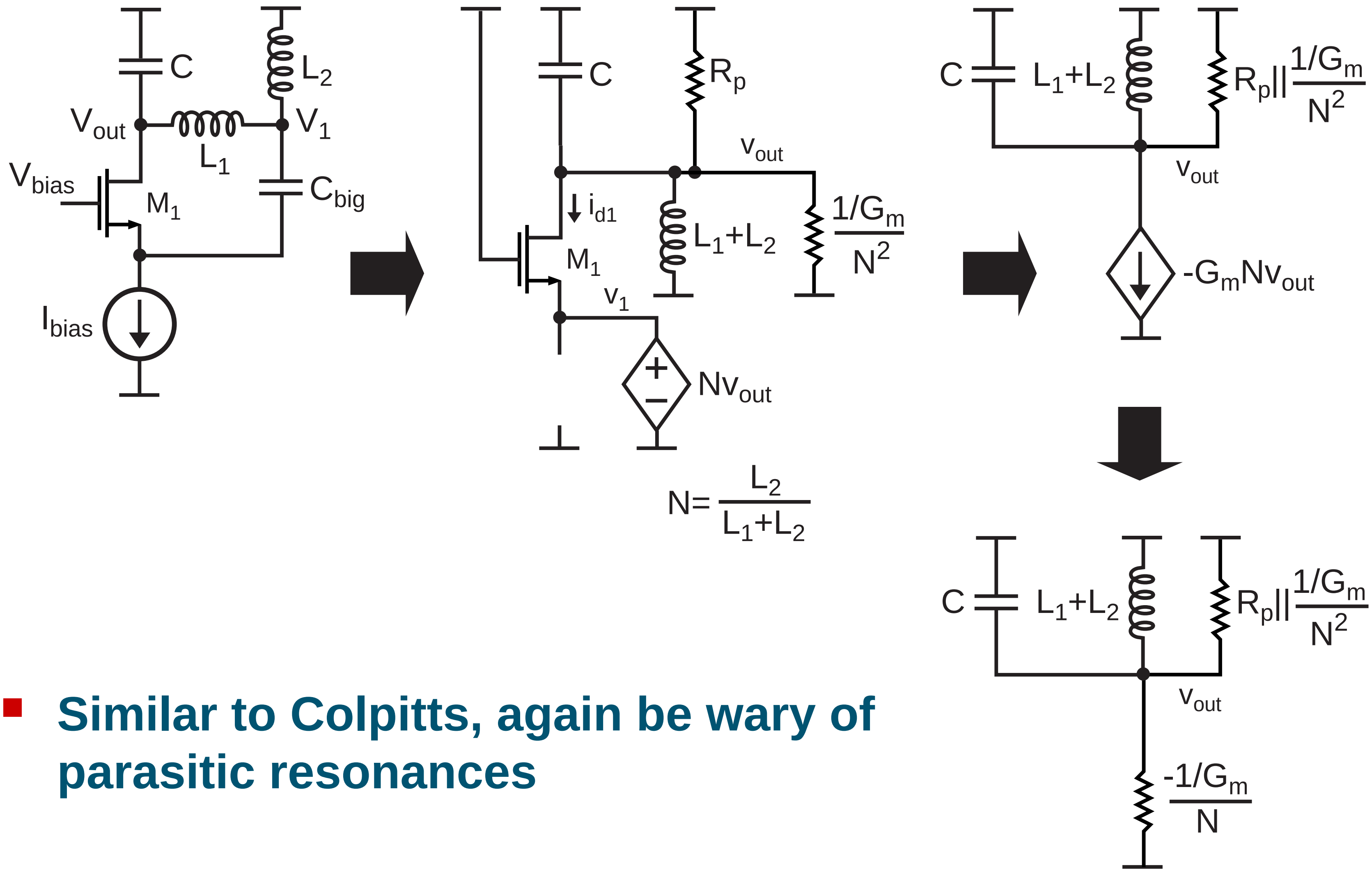


Hartley Oscillator



- **Same as Colpitts, but uses a tapped inductor rather than series capacitors to implement the transformer portion of the circuit**
  - **Not popular for IC implementations due to the fact that capacitors are easier to realize than inductors**

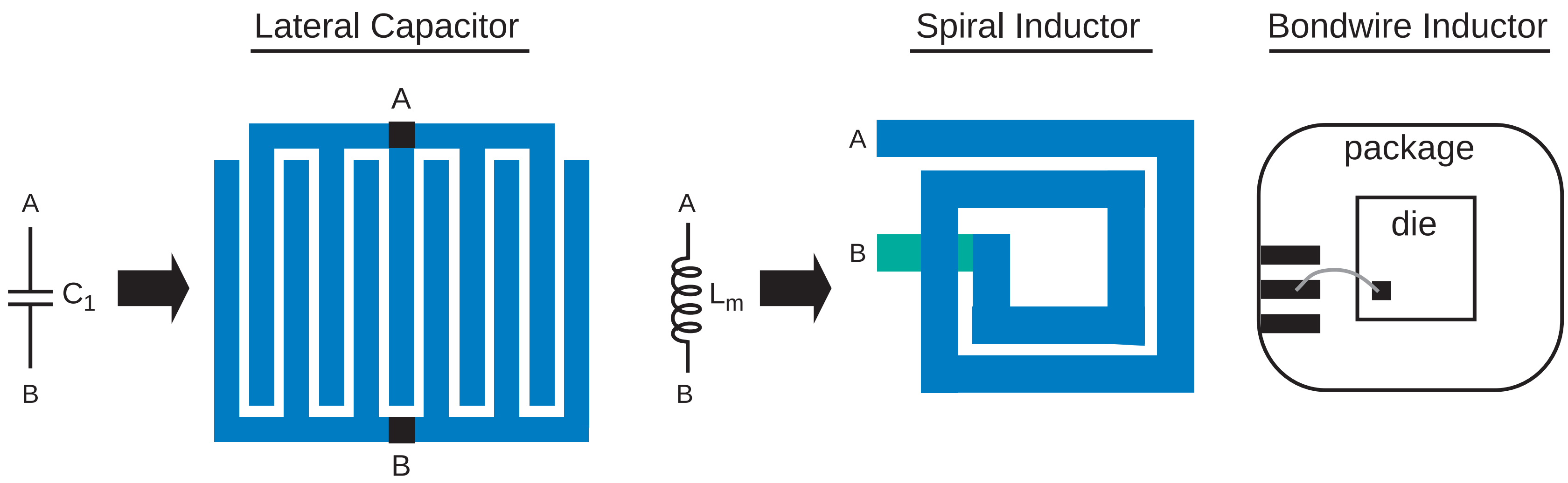
Simplified Model of Hartley Oscillator



- **Similar to Colpitts, again be wary of parasitic resonances**

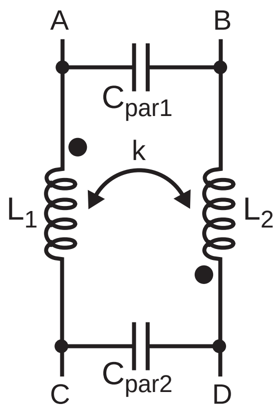
Integrated Resonator Structures

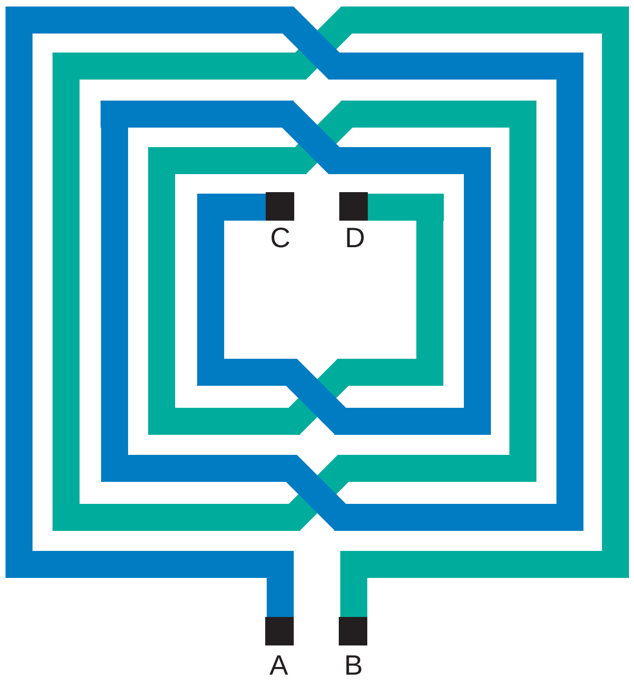
- **Inductor and capacitor tank**
  - **Lateral caps have high Q (> 50)**
  - **Spiral inductors have moderate Q (5 to 10), but completely integrated and have tight tolerance (< ± 10%)**
  - **Bondwire inductors have high Q (> 40), but not as “integrated” and have poor tolerance (> ± 20%)**
  - **Note: see Lecture 6 for more info on these**



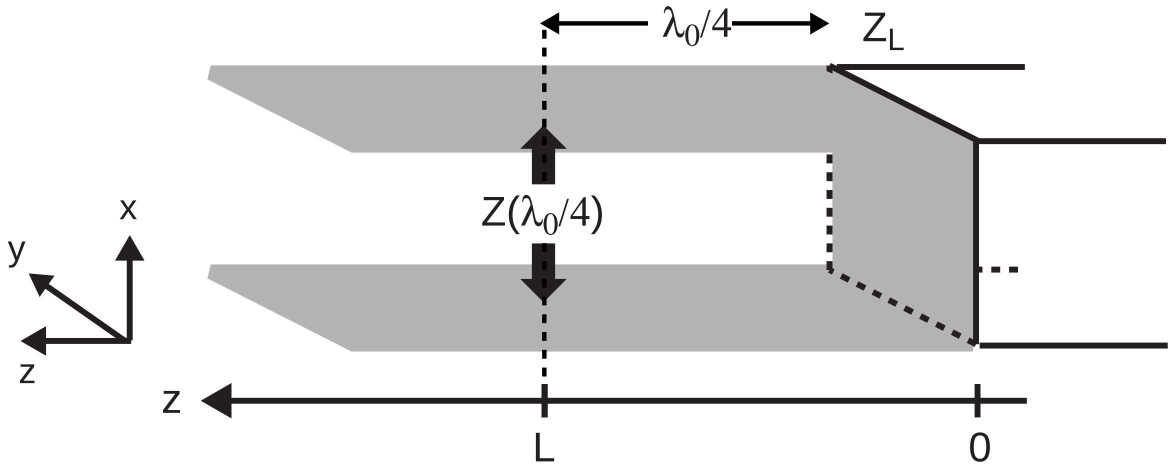
Integrated Resonator Structures

- **Integrated transformer**
  - **Leverages self and mutual inductance for resonance to achieve higher Q**
  - **See Straayer et. al., “A low-noise transformer-based 1.7 GHz CMOS VCO”, ISSCC 2002, pp 286-287**





Quarter Wave Resonator



- **Impedance calculation (from Lecture 4)**

$$Z(\lambda_o/4) \approx -j\frac{2}{\pi}\sqrt{\frac{L}{C}}\left(\frac{w_o}{\Delta w}\right)$$

  - **Looks like parallel LC tank!**
- **Benefit – very high Q can be achieved with fancy dielectric**
- **Negative – relatively large area (external implementation in the past), but getting smaller with higher frequencies!**

Other Types of Resonators

- **Quartz crystal**
  - **Very high Q, and very accurate and stable resonant frequency**
    - Confined to low frequencies (< 200 MHz)
    - Non-integrated
  - **Used to create low noise, accurate, "reference" oscillators**
- **SAW devices**
  - **Wide range of frequencies, cheap (see Lecture 9)**
- **MEMS devices**
  - **Cantilever beams – promise high Q, but non-tunable and haven't made it to the GHz range, yet, for resonant frequency**
  - **FBAR – Q > 1000, but non-tunable and poor accuracy**
  - **Other devices are on the way!**